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TWO-STATE POWER AMPLIFIER WITH TRANSITIONAL FEEDBACK

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ABSTRACT OF THE DISCLOSURE

A solid state amplifier using "on-off" mode power amplifying transistors fed with pulses from a multivibrator through pulse-width modulator means. The amplifier reproduces with good fidelity an input signal, for instance speech, which input signal modulates the amplified pulse widths from substantially zero for zero input amplitude to a maximum width wherein adjacent pulses blend together and produce a constant D.C. output level whenever the input signal reaches the maximum amplitude to which the system is responsive. In order to provide improved fidelity of reproduction, the system includes degenerative feedback across the whole amplifier, a degree of regenerative feedback in the pulse circuits to improve pulse response, and a special degenerative feedback across the pulse width modulator means which makes the pulses being amplified by the "on-off" mode amplifiers trapezoidal for the purpose of making the response smoother at zero crossings and at signal amplitude maxima by having the amplitudes of the pulses as well as their widths change at these extremes.

This invention relates to amplifier systems of the type in which the widths of pulses in a continuous chain of pulses are modulated in accordance with the amplitude of an input signal of lower frequency and then amplified by amplifiers operating in a switching mode, and more particularly this invention relates to improvements in the modulating circuitry for the purpose of improving the efficiency of the amplifier, and improving its linearity at instants when the amplitude of the input signal is very small, or when it is very large and approaching saturation.

This general type of amplifier system has in the past been referred to as a "two-state" amplification system, or as a "Class D" amplifier system, and examples of the general type of system appear in various forms in U.S. Patents 1,874,159; 2,969,506; 2,984,792; 2,990,516; 3,009,112; 3,112,365; and others. This general type of system is especially attractive in connection with amplifying input signals to relatively high power levels using power-amplifying semiconductor components operating between cut-off and saturation in "on-off" switching modes. The prior art points out the particular advantages involved in amplifying signals which have only two amplitude levels, as distinguished from signals having continuously variable amplitude levels. These two-level signals are especially attractive in connection with semi-conductor circuits since the amplification thereof is relatively insensitive to variations in semiconductor characteristics, especally linearity characteristics. Where "on-off" switching mode operation is employed, only the instants of zero crossovers are important, and since the semiconductors are switched from "off" condition to "on" condition almost instantaneously, the internal power dissipation in the semi-conductors is very small. The fact, in turn, makes it possible to use relatively smaller semiconductor ratings to deliver much greater maximum power in a two-level amplifier, than in a conventional amplifier.

This general type of amplification employs a square wave generator, such as a multivibrator, which continuously delivers alternating positive and negative pulses at a fixed frequency which is considerably higher than any input signal frequency to be amplified, and in the absence of an input signal these pulses are symmetrical about a zero axis so that their average value is zero. However, when an input signal is introduced, if its instantaneous value is positive, the pulses in the aforementioned chain on one side of the zero axis are lengthened in duration, and the pulses on the other side of the zero axis are shortened in duration, so that their average value is no longer zero but depends upon the polarity and magnitude of the instantaneous input signal. Conversely, a negative input signal results in shortening of the pulses on said one side of the axis and lengthening of the duration of the pulses on the other side of the zero axis so that the average value moves off of zero in the opposite direction. The peak amplitude of these pulses, however, does not change except in the vicinity of zero input signal conditions as will be explained below, and therefore the power amplifier is normally amplifying pulses of constant height, and therefore the power amplifiers themselves can conveniently be operated in an "on-off"-mode.

In this type of operation, the effeciency is very great because semi-conductors operating in the switching mode have very little internal power dissipation since their internal resistance, except during brief transitional periods is either virtually zero in the full-"on" condition, or effectively infinite in the full-"off" condition. In the past, using ordinary amplifying techniques, maximum efficiency obtainable was only about 75%, but in the two-state amplifier a practical working value of efficiency is about 95%. Moreover, because of smaller internal dissipation, a given semiconductor may safely deliver about five times the maximum power which it could deliver in an ordinary amplifying circuit. Thus, the dynamic range of this type of amplifier can be made greater without increase in distortion, and with excellent stability.

It is a major object of the invention to provide improved pulse-width modulating circuitry in which supersonic high-energy pulses from the multivibrator are first converted into two separate time-interlaced sawtooth waves which are then applied to two different modulator-amplifiers, each driving separate power amplifier paths, one for amplifying the positive components of input signals, and the other for amplifying the negative components thereof. Each amplifier is turned "on" by the steep leading edge of its associated sawtooth, but it is turned "off" when the level of the triangular trailing edge of the sawtooth augmented by any input signal component superposed thereon instantaneously falls below the level required to maintain the power amplifier "on," whereby the time duration of the "on"-condition of the amplifier is a function of the instantaneous input signal level, and the polarity of this input signal determines which of the two power amplifier paths is operative at any particular instant.

The principal advantage of the present pulse-width modulating circuit resides in improved efficiency obtainable with this circuit, particularly with regard to conservation of power under conditions of zero input signal, or small-amplitude input signals. Obviously, the efficiency of power consumption would be poor if, as in prior art circuits, the power transistors deliver the same amount of square-wave carrier power for all input signal amplitudes, as is the case if the only mode of modulation of the carrier pulses is width-modulation in which the positive and negative alternating pulses are of mutually complementary width always adding up to equal a constant amount of power. It is a major purpose of this invention to provide a modulator in which under zero input signal conditions, the modulator passes only very narrow alternating spikes which are easily filtered out. When a substantial input signal of one polarity is applied, these spikes on one side of the zero axis grow to be substantially square pulses of constant (saturation) height and having widths determined by the instantaneous amplitude of the input signal; and the spikes on the other side of the zero axis disappear altogether. The opposite set of spikes, however, will grow when the instantaneous polarity of the input signal reverses.

This type of system works very well except that it introduces certain discontinuities which occur in the vicinity of the zero-axis crossover and/or in the vicinity of maximum input signal amplitudes. There is a practical limitation to the variation of the switching point due to the fact that switching time itself is finite, which necessarily means that a discontinuity exists between the narrowest possible pulse from the pulse-width modulator, and no pulse at all; and this discontinuity shows up as distortion occurring near zero-signal input and saturation signal input, the distortion being especially noticeable for small input signals.

It is another major object of this invention to reduce the distorting effect of this discontinuity, and thereby substantially eliminate the distortion which it introduces, and this improvement is accomplished by employing pulse-amplitude modulation in addition to pulse-width modulation in the vicinity of the extremes of the input signals, namely in the vicinity of the zero-axis input-signal crossings, and/or in the vicinity of the maximum signal amplitude which can be amplified. In this way, at the moment when the pulses approach either zero width, or approach maximum width resulting in a continuous DC level, the narrow pulses, or the narrow space between pulses, changes both in width and in amplitude, rather than suddenly going from maximum amplitude to zero amplitude in an abrupt and discontinuous manner which will introduce appreciable distortion.

It is another major object of this invention to provide several different types of feedback paths in a two-state amplifier, these paths respectively providing: regenerative feedback across the pulse-width modulator to sharpen the pulse response thereof; a separate degenerative feedback path across the whole amplifier system to improve over-all linearity; and a novel, specially-controlled degenerative feedback path operating across the pulse-width modulator to make its output pulse shape slightly trapezoidal so that very narrow pulses will have triangular sides which will cause the amplitude thereof to shrink whenever the width of the pulse approaches zero or approaches continuous DC in the vicinity of saturation, thereby giving the aforementioned amplitude-modulation effect in the vicinity of zero-axis crossover and also in the vicinity of maximum output signal level.

As stated above the degenerative feedback applied across the modulator is limited in magnitude to such an extent that it strongly affects the pulses from the modulator only under zero and small input-signal conditions. In the absence of such feedback the narrow spikes occurring for zero input levels would be the same amplitude as the wider output pulses occurring in response to substantially greater input amplitudes. However, the degenerative feedback has a sizeable effect on these narrow spikes, first shrinking their amplitudes about 50% and then making them essentially triangular in shape for a zero input signal. If then a very small input signal is applied to the modulator, the spikes on one side of the zero axis further shrink and the opposite spikes grow. As the signal amplitude further increases, the former spikes disappear altogether as the latter spikes reach the full amplitude of the pulse output of the modulator, and, upon further increase in input amplitude the latter spikes grow wider and wider until at the maximum useful input amplitude, the output of the modulator is a DC level in which the space between pulses has vanished. In the last stages of disappearing, this space between pulses becomes triangular (spike-shaped) due to the special degenerative feedback and then shrinks upwardly toward the ultimate DC level. Thus, it will be seen that the amount of power consumed by the amplifier system is essentially proportional to the instantaneous input amplitude and is very small for zero and for small input amplitude levels.

It is another important object of this invention to provide a system in which the pulse repetition frequency is more efficiently filtered out because the total amount of carrier power delivered by the power output amplifier to the filter is very small for small input signal amplitudes. To the extent that the filter is imperfect, some of the carrier (pulse) frequency will be delivered to the load as spurious energy, and it is much easier to filter out this energy in the present system where it is small in the vicinity of zero-input signal, than in prior art systems where this energy is as great for zero input as it is for greater input signal levels.

Other objects and advantages of the invention will become apparent during the following discussion of several practical embodiments of the invention, which has been built and succesfully tested. Reference is made to the drawings, wherein:

FIG. 1 is a schematic diagram of a preferred embodiment of the present invention;

FIG. 2 is a graphical illustration of the interlaced sawtooth waves applied through coupling resistors to the pulse-width modulators shown in the schematic diagrams;

FIG. 3 is a graphical illustration showing an improvement which can be made in the sawtooth waves applied to the width modulators;

FIG. 4 is a graphical illustration of the effect of the special limited-amplitude negative feedback provided for the purpose of limiting the output of a pulse-width modulator under zero-input-signal conditions to about half its normal output pulse height, and for making such output pulses slightly triangular in shape so that they will be amplitude-modulated by very small input signals at the terminal **25**;

FIG. 5 is a graphical illustration showing encircled some typical output waveforms of a modulator system not equipped with the amplitude-controlled negative feedback system according to the present invention;

FIG. 6 is a graphical representation similar to FIG. 5 but showing the effect of the amplitude-controlled negative feedback circuit as applied to signal levels in the vicinity of zero-axis crossover and saturation input signal level;

FIG. 7 is a schematic diagram of a power output stage, modified with respect to the output stage of FIG. 1;

FIG. 8 is a showing of a modification of the input amplifier stages of the system shown in FIG. 1;

FIG. 9 is a schematic diagram illustrating a modified form of pulse-width modulator in which two transistor stages have been eliminated as compared with FIG. 1;

FIG. 10 is a schematic diagram of a considerably modified amplifier system employing NPN transistors except in the power amplifier stage; and

FIG. 11 is a further modification similar to FIG. 10 but simplified to omit several transistors employed in the FIG. 10 modification.

Referring now to FIG. 1 of the drawings, this figure shows a preferred working embodiment of the invention including four basic circuit portions:

First, there is an input circuit including the transistor **T1** which receives the signal to be amplified and splits it into two opposed phases which are then delivered to linear audio amplifiers including transistors **T2** and **T3**.

Second, the system includes a free-running multivibrator circuit including the transistors **T4** and **T5** which continuously oscillate at a supersonic rate and thereby deliver a carrier frequency in the form of large energy-content pulses.

Third, the system includes a pulse-width modulator circuit comprising transistors **T6** and **T7** which receive outputs from the above-mentioned multivibrator, and also receive phase-split components of the input signal which is to be amplified; and these modulator transistors **T6** and **T7** deliver outputs which drive the fourth circuit portion, namely "on-off" power amplifiers. An amplitude-controlled negative feedback transistor **T8** is provided for the novel purpose hereinafter discussed, and this transistor is in a feedback path connected operatively across the pulse-width modulator circuit.

The power amplifier circuit which comprises the fourth circuit portion includes two driver transistors **T9** and **T10** which are direct-coupled to drive the final power amplifier transistors **T11** and **T12**. The transistors **T9**, **T10**, **T11** and **T12** are all normally cut "off," and these transistors are turned "on" by the modulator outputs at appropriate moments and in such a manner as to drive the power transistors usually to saturation, so that the power transistors operate in a two-state "on-off" switching mode.

Discussing these four circuit portions of the system in further detail, the carrier frequency generator **1** comprises a free-running multivibrator circuit of conventional design in which the capacitors **2** and **3** when considered with the resistors **4**, **5**, **6**, and **7** provide a supersonic time constant in a manner well-known per se. The emitters of the transistors are returned directly to the positive supply labeled B+ and the collectors of the transistors are returned through the resistances **4** and **7** to the other side of the power supply labeled B−. The resistors **5** and **6** supply a small forward bias to the bases of the transistors and from which the above-mentioned large energy-content pulses are taken through diodes **8** and **9**, which alternately supply positive pulses to charge capacitors **10** and **11**. The charge on the capacitor **10** produced by any particular pulse from the multivibrator leaks off along an approximately sawtooth waveform shown in FIG. 2 and labeled **10′**, this charge passing through the resistor **12** and upwardly through the resistor **13**. Bias current supplied through the resistor **14** renders the transistor **T6** conductive most of the time, but when the sawtooth current through the resistor **13** exceeds this bias in the resistor **14**, transistor **T6** is cut "off." The capacitor **15** merely serves to make the leading edge of the sawtooth wave **13′** sharper as shown in FIG. 3, and in a manner well-known in the pulse handling art. Likewise, on alternate half cycles of the multivibrator **1**, the capacitor **11** is charged positively and this charge leaks off along the curve labeled **11′** in FIG. 2 to produce another approximately sawtooth waveform interlaced in time with the waveform **10′**. This charge leaks through the resistance **16**, and through the resistance **17** to oppose the forward bias supplied the transistor **T7** through the resistance **18**. The capacitor **21** serves a purpose similar to the capacitor **15**. Thus, alternate positive sawtooth waves are applied to the transistors **T6** and **T7** at the points labeled **19** and **20**, for the purpose to be explained more fully hereinafter.

The input signal to be amplified in the present system is applied at an input terminal **25**, FIG. 1, and for illustrative purposes it will be assumed that the input waveform is a sine wave. An impedance Z is illustrated to represent the internal impedance of the source of the input signal S. This input signal passes through a capacitor **26** and is applied to the base of the transistor **T1** which is forward-biased by the resistor **27** in a manner well-known per se. The output impedance of the transistor **T1** is equally divided between the collector circuit and the emitter circuit, and takes the form of equal load resistances **28** and **29**, so that the output of the transistor **T1** is in the same form as the input signal S, but includes two oppositely phased signals which are passed through the capacitors **30** and **31** and through the resistors **32** and **33** to the bases of the transistors **T2** and **T3**. These transistors amplify the phase-split components of the input signal and deliver outputs respectively through the resistances **14** and **18** to the bases of the modulator transistors **T6**

and **T7**. The transistors **T2** and **T6** are direct-coupled, as is also the case with the transistors **T3** and **T7**, and the load resistances **34** and **35** of the transistors **T2** and **T3** when taken with the resistors **14** and **18** form voltage-divider chains which are so proportioned as to maintain the transistors **T6** and **T7** fully saturated and conductive in the absence of any input signals, whether signals from the terminal **25** or pulses from the multivibrator **1**. Thus, since these are PNP transistors, a positive signal at point as to render transistors **T6** and **T7** fully conductive, and since these are PNP transistors, a positive signal at point **19** or **20** tends to turn the corresponding transistor "off."

On alternate half cycles of the multivibrator **1**, large positive sawtooth voltages are applied with steep leading edges to points **19** and **20**, respectively, as shown in FIG. 2 in connection with the illustrated waves **10′** and **11′**. The transistor **T6** is momentarily cut "off" by the leading edge of the sawtooth wave **10′**, but in the absence of an input signal, this charge leaks off from the capacitor **10** and soon falls below a sufficient level to overcome the forward bias on the transistor **T6** thus allowing it to regain conductivity after only a brief "off" interval. The same sequence occurs on opposite half cycles of the multivibrator **1** with respect to the transistor **T7** which is briefly cut "off" by the sharp positive leading edge of the sawtooth wave **11′**, which charge leaks off from the capacitor **11** through the resistance **16**, permitting the transistor **T7** to regain conductivity after only a brief "off" interval, assuming no input signal to the terminal **25**.

It should be briefly stated here that the power amplifiers **T9** and **T11**, and **T10** and **T12**, are normally con-conductive when the modulator transistors **T6** and **T7** are (normally) conductive. Therefore, during the "off" intervals of the modulators, the power amplifiers are switched to "on" condition to thereby deliver an output to the load L. This will be further discussed below.

Returning to the discussion of transistor **T6**, as stated above after the leading edge of the sawtooth **10′** cuts "off" the transistor **T6** it will return to conductive state after only a little of the charge has leaked from capacitor **10**, and during the "off" interval it progressively becomes easier for the transistor **T6** to regain conductivity as the sawtooth decays through the resistor **13** and the resistor **14**. Although the resistance values are so proportioned that the transistor **T6** would normally regain conductivity by the time the sawtooth wave has decayed slightly, there may also be applied to the point **19** an amplified component of the input signal S. If the momentary value of the signal S is positive at the input terminal **25**, the signal at the capacitor **30** will be negative, but the signal at the resistor **14** will be positive. This positive component at resistor **14** is supplied to the transistor **T6** so as to augment the positive sawtooth, and thus increase the duration of the transistor "off" time by driving it further beyond cut-off. At maximum positive input signal the combined signal component and the sawtooth component will prevent it from regaining conductivity at all during the decay of the sawtooth, thus producing an output of maximum duration to the load by the power transistors **T9** and **T11**. On the other hand, the oppositely-phased component of the input signal S applied through the transistor **T3** and the resistance **18** will be negative in value at the resistor **18** and will therefore buck the positive sawtooth current applied at the point **20** through the resistance **17**. Since the positive sawooth **11′** at point **20** is barely able to cut "off" transistor **T7**, even a small negative signal component at point **20** will tend to overcome the sawtooth current and allow the transistor **T7** to remain conductive. Thus, little or no output to the load L will be delivered by the power transistors **T10** and **T12** which will remain "off" when the transistor **T7** remains "on." A very small negative signal component applied through the resistor **18** may not quite overcome the positive sawtooth applied to the transistor **T7**, but a slightly larger negative signal component will overcome it entirely. Thus, when a positive signal is applied to input terminal **25**, transistor **T6** drives power amplifiers **T9** and **T11** to deliver an output pulse whose duration depends on the amplitude of the input signal, but the oppositely-phased component of input signal bucks the sawtooth applied to transistor **T7** and prevents it from cutting off **T7** at all if the input is more than very small in amplitude. In general, an input to terminal **25** of positive value turns "on" the power amplifiers **T9** and **T11**, and maintains amplifiers **T10** and **T12** "off." Conversely, a negative input to terminal **25** turns "on" power amplifiers **T10** and **T12**, but maintains **T9** and **T11** "off." With zero-signal input **T9** and **T11** conduct very briefly at the peaks of the sawteeth **10'**, and **T10** and **T12** conduct very briefly at the peaks of sawteeth **11'**. A very small positive input shrinks the output from **T10** and **T12** and widens the interval of conductivity of **T9** and **T11** proportionately. As the input amplitude increases, the former shrinks more and approaches zero, while the latter grows, approaching continuous conduction for saturation level positive input signals. The opposite conductivity conditions occur when a negative signal is applied to the input terminal **25**. A small amount of regenerative feedback is provided through the resistances **38** and **39** for the purpose of sharpening the response of the transistors **T6** and **T7** to input signals so as to provide very rapid and steep-acting characteristics. The capacitors **40** and **41** further sharpen this action in a manner well-known per se.

The modulator transistors **T6** and **T7** are provided respectively with load resistors **45** and **46**, and since the transistors **T6** and **T7** are normally conductive their normal output level is positive at the collectors and this positive signal is directly applied through the resistors **47** and **48** to the bases of the driver transistors **T9** and **T10**. Capacitors **49** and **50** sharpen the response to the outputs from transistors **T6** and **T7**.

The transistors **T9** and **T10** are directly connected to the transistors **T11** and **T12**, respectively, as emitter follower stages for driving these power transistors. The fact that the transistors **T6** and **T7** are normally conductive and therefore normally deliver a positive output maintains the PNP transistors **T9**, **T10**, **T11** and **T12** nonconductive. On the other hand, when one of the transistors **T6** or **T7** is driven "off" by one of the sawtooth waves **10'** or **11'** the collector of that modulator transistor goes sharply negative and pulses the associated drive and power transistor to saturation. Thus, when the transistor **T6** is "on," the transistors **T9** and **T11** are "off," and vice versa. This same statement is also true of transistor **T7**, and of its control action as applied to the transistors **T10** and **T12**.

The collectors of the power transistors **T11** and **T12** are connected in push-pull to taps **52** and **53** of output transformer **51** having a center tap **54** connected with the B-supply. The load is taken off across the outermost terminals **55** and **56**, and in the illustrative practical working embodiment including circuit components tabulated below, the windings are such as to drive a load L of 16 ohms. The leakage inductance of the winding of the transformer taken with the capacitors **57** and **58** produces an LC filter which is tuned to eliminate the supersonic carrier frequency generated by the multivibrator **1** and smooth the output load to regain a waveform similar to the input waveform at terminal **25** but greatly amplified. A quantity of negative feedback is applied from the power transistor stage output through the wire **60**, the resistances **61** and **62**, and the wire **63** in order to improve the linearity of the amplifier system's response, the capacitors **64** and **65** serving further to filter out any remaining supersonic carrier frequency.

The transformer connections for a load L impedance greater than the transistor impedance is shown in FIG. 1, but where the load L' has an impedance less than that of the transistors, the circuit of FIG. 7 should be used in which the transistors **T11** and **T12** have their collectors connected to the ends **155** and **156** of the transformer **151** winding, and the supply-power is fed into the center tap **152** while the load L' is connected across intermediate taps **152** and **153**. The filter capacitors **157** and **158** are still across the load L' but must be of greater capacity since the winding has less inductance. It is, of course, not necessary that the transformers **51** and **151** be auto-transformers.

As mentioned above, with zero input signal S at terminal **25** the modulators **T6** and **T7** deliver very narrow alternate pulses to turn on the power amplifiers. Without a special degenerative feedback circuit, a small input signal would cause one polarity of these pulses to disappear, and there would always be an abrupt transition from a narrow pulse to no pulse at all, which would result in a discontinuity occurring each time the input signal crossed its zero axis. The present invention provides novel means for eliminating this discontinuity by making these alternate positive and negative pulses, when they become very narrow in width, shrink also in amplitudes as well as pulse-width in the vicinity of zero-axis crossings of the input wave. This is accomplished by providing a special feedback circuit which includes the transistor **T8**, and the resistors **68**, **69** and **70**. The resistor **70** is connected in series between the B− supply and the load resistors **34** and **35** of the input signal amplifiers **T2** and **T3**. When the transistor **T8** is nonconductive the resistor **70** in series with the load resistors **34** and **35** somewhat reduces the flow of current through them.

When transistor **T8** is fully conductive, however, resistor **70** is effectively shorted, thus increasing the forward bias of transistors **T6** and **T7**. If **T8** is less than fully conductive, then there will be only a partial increase in forward bias of transistors **T6** and **T7**. The collectors of the transistors **T9** and **T10** are substantially directly returned to the B− supply through the small resistor **68** so that they are connected in common-collector-configurations. These transistors are normally "off," and therefore no voltage appears across the resistance **68** inserted in series with these collectors. However, when one of the transistors **T9** or **T10** is suddenly rendered conductive by negative pulses **47'** or **48'**, FIG. 4, applied through resistor **47** or **48** as a result of the associated modulator transistor **T6** or **T7** being turned "off," a positive pulse of voltage **68'**, as shown in FIG. 4, is developed at point **72**, and coupled through the limiting resistance **69** to the base of NPN transistor **T8**, thereby pulsing it partially conductive and partially short-circuiting the resistance **70** for the duration of the pulse **68'**. Accordingly, the voltage drop which had been introduced in series with the load resistors **34** and **35** by resistor **70** disappears, thereby rendering these resistors more negative, which places degenerative feedback on the inputs to the two normally "on" modulator transistors **T6** and **T7**, bucking the positive sawtooth waves applied thereto and turning them back "on" sooner, so as to reduce their output signals and thereby turning "off" the power amplifiers sooner. The amount of feedback is limited by the size of the voltage drop across resistor **70** when transistor **T8** is cut "off," and the magnitude of resistor **70** therefore determines the maximum magnitude of the thus controlled negative feedback, and the amount of negative feedback determines how much the narrow pulses from the power amplifier are reduced in amplitude as compared with wider output pulses from the power amplifiers.

For small signal inputs the duration for which the sawtooth pulses transistor **T6** or **T7** "off" varies and thus causes the magnitude of negative feedback through resistor **69** and transistor **T8** to change the voltage dropped across resistor **70** varies. As pulses are increased in the one polarity the feedback increases until, at approximately the point where output pulse reaches full saturation amplitude, resistor **70** is completely short-circuited by transistor **T8**. In the other polarity, at the same point in the signal waveform, the transmitted pulse reaches zero amplitude, transistor **T8** does not conduct at all during the equivalent pulse period, and resistor **70** develops its maximum voltage drop for that moment.

Referring now to FIGS. 5 and 6, FIG. 5 shows the operation of the present amplifier system without the negative feedback provided by the transistor **T8** and the resistors **68**, **69** and **70**; whereas the diagram of FIG. 6 shows the operation of the system when this negative feedback is present. The circled waveforms represent the unfiltered output of the system for the various input signal amplitudes indicated. By comparison of the two diagrams, it can be seen that this negative feedback provides amplitude modulation of the pulses occurring at the instants of extreme input signal levels, i.e., either near the operation of an amplifier system which is strictly two-state, meaning that if a pulse X is present in the output at all, it is of full amplitude, but by contrast FIG. 6 shows how, by making the pulse trapezoidal, a spike Y is made triangular so that it diminishes gradually in amplitude just before it disappears altogether in the present novel system. FIG. 6 also shows the manner in which the triangular spiked pulses Y diminish in magnitude on one side of the zero-axis and increase in magnitude as at Y′ on the other side of the zero-axis, until the diminishing spikes disappear completely and the increasing spikes turn into full square waves which, although still slightly triangular on their sides, do not visibly show it.

FIG. 8 shows a modification of the input stages preceding the modulators. Parts in FIG. 8 which are similar to those in FIG. 1 bear similar reference numerals, but with a prefix 200 added to the reference numerals. The phase-splitter transistor **T1** is shown in FIG. 8 as having respective collector and emitter load resistors **228** and **229** delivering outputs through capacitors **230** and **231**. In FIG. 1, there are two series-connected resistors **32** and **33** which are inserted for the purpose of providing the same effective input impedance to transistors **T2** and **T3** as the load impedances **228** and **229** of the phase-splitter **T1**. In FIG. 8, there are no resistors corresponding with resistors **32** and **33** of FIG. 1, but instead resistors **222** and **223** are inserted in the emitters of the amplifiers **T2** and **T3** to increase the input impedances to these amplifiers **T2** and **T3**, and since they are not bypassed, they provide a certain amount of degenerative feedback which helps to maintain the linearity of the amplifier stages. This is a workable alternative, although the circuit shown in FIG. 1 is believed to be preferable in view of the fact that the resistors **32** and **33** are themselves more linear than the inputs to the transistors **T2** and **T3** in FIG. 8. Moreover, the circuit in FIG. 8 requires more precise biasing of the transistors in order to maintain satisfactory linearity. It is another advantage of the circuit of FIG. 1 that the presence of the resistors **32** and **33** provides isolation of the feedback pulses presented through resistances **38** and **39**. In other words, the resistors **32** and **33** reduce the tendency of the feedback pulses through the resistor **39** to be applied to the base of transistor **T2**, and the tendency of the pulses fed back through the resistor **38** to find their way to the base of transistor **T3**.

FIG. 9 shows still another modification of the system of FIG. 1 which has been simplified by the omission of transistors **T2** and **T3**, the modified circuit being suitable where less overall gain is required. The modification of FIG. 9 has had the prefix 300 placed before each reference numeral which designates a part performing similarly as it performed in FIG. 1. Transistor **T1** is still a phase-splitter providing oppositely-phased signals which are delivered through blocking capacitors **330** and **331** to the transistors **T6** and **T7**, the transistors **T2** and **T3** having been eliminated. In the circuit shown in FIG. 1, the transistors **T2** and **T3** and their load resistances **34** and **35** provided the necessary bias levels on the bases of the transistors **T6** and **T7** in order to maintain them normally-conductive. Since the blocking capacitors **330** and **331** isolate the bases of the transistors **T6** and **T7** in FIG. 9, forward-bias resistors **380** and **381** provide the sole control of current fed to the bases of the transistors **T6** and **T7** in the absence of the sawtooth. While the resistors **34** and **35** of FIG. 1 must carry both bias current for **T6** and **T7** and collector current for **T2** and **T3**, in FIG. 9 resistors **380** and **381** carry only the bias current for **T6** and **T7**, thus giving more precise control. The driver transistors **T9** and **T10** have been provided with additional and separate load resistors **374** and **375**, and positive feedback is taken from the junctions of the collectors of **T9** and **T10** with these load resistors. Thus, two transistor stages can be saved where total gain need not be as great, without, however, changing the mode of operation of the amplifier and modulator circuits.

FIG. 10 represents a more extensive modification of the system for the purpose of showing how NPN transistors can be used in connection with the low-level amplifier, and the modulating stages, although PNP transistors are still illustrated for the final power amplifier and driver stages. Reference numerals which designate parts performing functions which are analogous to the functions performed by parts shown in FIG. 1 are provided with similar reference numerals but with the prefix 400 added before each of the numerals. The input stage **T41** is an NPN transistor which still performs a phase-splitting function so as to deliver oppositely-phased signal components through the capacitors **430** and **431** to the amplifier transistors **T42** and **T43**. These transistors are provided with load resistances **434** and **435** which deliver outputs through the resistors **414** and **418** to the bases of modulator transistors **T46** and **T47**. The resistors **434** and **435** also provide the normal saturation bias to the bases of the modulators **T46** and **T47**. In the system shown in FIG. 10, the multivibrator **401** delivers negative interlaced sawtooth waves through diodes **408** and **409** and resistances **413** and **417**. The normally-"on" transistors **T46** and **T47** are shut "off" by these negative sawteeth, and thereby bias the normally "off" transistors **T49** and **T50** "on." Whenever either transistors **T49** and **T50** is turned "on" it will bias the associated driver transistor **T51** or **T52** also "on," the transistors **T49** and **T50** being directly coupled to the complementary transistors **T51** and **T52**, the former being NPN transistors and the latter being PNP transistors. The transistors **T51** and **T52** serve as current amplifiers to provide sufficient drive to the bases of the transistors **T53** and **T54**, which are coupled to the output transformer **451** by an emitter-coupled circuit, as distinguished from the collector-coupled circuit shown in FIG. 1. The resistors **484** and **485** are coupled with the emitters of the transistors **T51** and **T52** in a circuit which is analogous to that shown in FIG. 9 in order to drive the controlled-amplitude negative-feedback transistor **T48** for the purpose of providing the novel amplitude modulation of the pulse waveform in the vicinity of the zero-axis crossovers of the input signal S, and in the vicinity of maximum amplitudes of the input signal S, in a manner analogous to that described in connection with FIG. 1.

FIG. 11 shows a further modified combination of NPN transistors in the input and modulating stages, the present modification being especially useful where less overall gain is required since this circuit omits some of the transistors appearing in FIG. 10. In particular, this modification omits transistors **T46** and **T47** which appeared in FIG. 10 and uses the equivalent of the transistors **T49** and **T50** as pulse-width modulators. Parts shown in the diagram of FIG. 11 which are analogous in function to parts shown in FIG. 1 bear similar reference characters except for the addition of the prefix 500 to each reference numeral.